

Implementation of Super-Twisting Control: Super-Twisting and Higher Order Sliding Mode Observer Based Approaches

Asif Chalanga, *Member, IEEE*, Shyam Kamal, *Member, IEEE*, Leonid M. Fridman, *Member, IEEE*, Bijnan Bandyopadhyay, *Senior Member, IEEE*, Jaime A. Moreno, *Member, IEEE*,

Abstract—In this paper, an output feedback stabilization of perturbed double integrator systems using super-twisting control (STC) is studied. It is shown that when STC is implemented based on super-twisting observer (STO) then it is not possible to achieve second order sliding mode (SOSM) using continuous control on the chosen sliding surface. Two methodologies are proposed to circumvent the above mentioned problem. In the first method, control input is discontinuous which may not be desirable for practical systems. In second method continuous STC is proposed based on higher order sliding mode observer (HOSMO) which achieves SOSM on the chosen sliding surface. For simplicity, we are considering here only the perturbed double integrator, which can be generalized for an arbitrary order. Numerical simulations and experimental validation are also presented to show the effectiveness of the proposed method.

Index Terms—Super-twisting control (STC), super-twisting observer (STO), higher order sliding mode observer (HOSMO).

I. INTRODUCTION

SLIDING MODE CONTROL (SMC) [1]- [15] is one of the most promising robust control techniques. It is able to reject bounded matched perturbation theoretically completely. The main disadvantage of SMC is chattering [1]- [3].

To avoid the chattering effect, several methodologies are proposed in sliding mode literature, STC [16] is one among them. The STC plays a special role among the sliding mode controllers. Unlike other second order sliding mode (SOSM) controllers, STC is applicable to a system (in general, any order) where control appears in the first derivative of the sliding variable. It has following advantages:

- compensates uncertainties/perturbations that are Lipschitz¹;
- requires only information of the output (sliding variable) σ ;
- provides finite-time convergence to the origin for σ and $\dot{\sigma}$ simultaneously;
- generates continuous control signal and, consequently, adjusts the chattering;

For example if we want to apply STC on second order mechanical system to adjust the chattering problem then we have to design a sliding variable such that it has relative degree one. If we choose a linear surface then STC ensures the uncertainties/perturbations compensation, finite time convergence to sliding variable and its derivative, but states converges *asymptotically* to the origin.

The sliding mode approach has been exceptionally successful in the design of state feedback controllers. However, in most of the physical systems, an output is available for measurement. In that case, other states of the system can be obtained using an observer. The sliding mode observers are widely used due to the finite time convergence, insensitive with respect to uncertainties and also the estimation of the uncertainty [21].

A new generation of observers, based on the cascaded interconnection of the super-twisting algorithm (STA) have been recently developed [22], [18]. The STA is a well known SOSM algorithm introduced in [17] and it has been widely used for control, observation [22] and robust exact differentiation. Finite time convergence and robustness for the STA has been proved by geometrical methods [16] and by means of Lyapunov based approach [19], [20].

An output feedback finite time stabilization for a double integrator system using observer is already studied in the [26]- [28]. The controller used in [26]- [28] are able to achieve finite time stabilization of the states only when system is free from the disturbance. These controllers are not able to reject disturbance theoretically completely in the case of disturbance, so the states will be remain bounded around origin in the case of disturbance and bound depends on magnitude of the disturbance.

Using output feedback, twisting control [25] and prescribed control law it is possible to achieve finite time stabilization

¹First-order sliding-mode can compensate also discontinuous and uniformly bounded uncertainties/perturbations.

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Asif Chalanga and B. Bandyopadhyay are with the IDP in Systems and Control Engineering, Indian Institute of Technology Bombay, Mumbai 400076, India (e-mail: asif@sc.iitb.ac.in, bijnan@ee.iitb.ac.in)

Shyam Kamal is with Department of Systems Design and Informatics, Kyushu Institute of Technology, Japan (e-mail: kamal@ces.kyutech.ac.jp)

Leonid Fridman is with Institut für Regelungs- und Automatisierungstechnik 8010 Graz, Kopernikusgasse 24/II, Austria, on leave of Departamento de Ingeniería de Control y Robótica, División de Ingeniería Eléctrica, Facultad de Ingeniería, Universidad Nacional Autónoma de México, Ciudad Universitaria D.F., Mexico (e-mail: lfridman@unam.mx)

J. A. Moreno is with the Eléctrica y Computación, Instituto de Ingeniería, Universidad Nacional Autónoma de México (UNAM), 04360 México, D.F., Mexico (e-mail: JMorenoP@ii.unam.mx).

of both the states of perturbed double integrator system. But, the control input is discontinuous in nature and it generates chattering, which is undesirable. Using STC we can stabilize both the states of the perturbed double integrator asymptotically using continuous control. Due to continuous control STC [29], [30] can adjust the chattering problem which is good from the practical point of view.

A. Main Contribution

If only output is available for perturbed double integrator system and STC is to be designed then we need both states information. Using STO it is possible to estimate other state in finite time in the presence of disturbance. It is shown in the paper that when STC is implemented based on STO then it is not possible to achieve SOSM using continuous control on the chosen sliding surface. In this paper two methodologies are proposed to circumvent the above problem. In the first method, control input is discontinuous which may not be desirable for practical systems. In second method continuous STC is proposed based on HOSMO which achieves SOSM on the chosen sliding surface. For simplicity, we are considering here only the perturbed double integrator, which can be generalized for an arbitrary order.

B. Structure of the Paper

The paper is organized as follows. Section II discusses the STC based on STO for perturbed double integrator system. Section III details the super-twisting output feedback (STOF) control. HOSMO based STC for perturbed double integrator is discussed in Section IV. Section V contains application of proposed method to an industrial plant emulator followed by the concluding Section.

II. STC BASED ON STO FOR PERTURBED DOUBLE INTEGRATOR SYSTEM

Consider the dynamical system of the following form

$$\begin{aligned}\dot{x}_1 &= x_2 \\ \dot{x}_2 &= u + \rho_1 \\ y &= x_1,\end{aligned}\quad (1)$$

where y is an output of the system and ρ_1 is a disturbance. Only output information is available here, most of the controller needs the all state information, so first we reconstruct the other state of the system and then we design the STC based on the estimated information. STO is already reported in the literature [22], using that, next we will show that the STC design based on STO does not have a mathematical justification.

The STO dynamics to estimate the states of the system (1) is given in the following form

$$\begin{aligned}\dot{\hat{x}}_1 &= z_1 + \hat{x}_2 \\ \dot{\hat{x}}_2 &= z_2 + u,\end{aligned}\quad (2)$$

where z_1 and z_2 are the correction terms. Let, define the error variable as $e_1 = x_1 - \hat{x}_1$ and $e_2 = x_2 - \hat{x}_2$. The correction terms are selected as $z_1 = k_1|e_1|^{\frac{1}{2}}\text{sign}(e_1)$ and

$z_2 = k_2\text{sign}(e_1)$. Then, we can represent error dynamics in the following form

$$\begin{aligned}\dot{e}_1 &= -k_1|e_1|^{\frac{1}{2}}\text{sign}(e_1) + e_2 \\ \dot{e}_2 &= -k_2\text{sign}(e_1) + \rho_1.\end{aligned}\quad (3)$$

It is assumed that $|\rho_1| < \Delta_0$. If we choose $k_1 = 1.5\sqrt{\Delta_0}$ and $k_2 = 1.1\Delta_0$ then the error e_1 and e_2 both will go to zero simultaneously. The above equation's finite time stability is already proved in the literature [20], [22] so we can conclude, e_1 and e_2 both will converge to zero in finite time $t > T_0$. Once the error e_1 and e_2 is zero, we can say that $x_1 = \hat{x}_1$ and $x_2 = \hat{x}_2$ after finite time $t > T_0$.

Now, for the controller design here an output of the system (1) has a relative degree two, therefore one cannot apply direct STC, because STC is applicable for only relative degree one system. Therefore, we have to define a sliding manifold of the following form to get a relative degree one

$$\hat{s} = c_1x_1 + \hat{x}_2 \quad \text{where } c_1 > 0. \quad (4)$$

To synthesize the control law (for designing STC), taking the time derivative of (4), then we can write as

$$\begin{aligned}\dot{\hat{s}} &= c_1\dot{x}_1 + \dot{\hat{x}}_2 \\ \dot{\hat{s}} &= c_1x_2 + u + k_2\text{sign}(e_1)\end{aligned}\quad (5)$$

Substituting the $x_2 = e_2 + \hat{x}_2$ in the (5), further we can write as

$$\dot{\hat{s}} = c_1\hat{x}_2 + c_1e_2 + u + k_2\text{sign}(e_1). \quad (6)$$

Now, transforming the system (1) in the co-ordinate of x_1 and \hat{s} by using (4) and (6) which can be written as

$$\begin{aligned}\dot{x}_1 &= \hat{s} - c_1x_1 + e_2 \\ \dot{\hat{s}} &= c_1\hat{x}_2 + c_1e_2 + u + k_2\text{sign}(e_1).\end{aligned}\quad (7)$$

Now, if we select the control u to get SOSM on \hat{s} as,

$$u = -c_1\hat{x}_2 - \lambda_1|\hat{s}|^{\frac{1}{2}}\text{sign}(\hat{s}) - \int_0^t \lambda_2\text{sign}(\hat{s})d\tau, \quad (8)$$

where λ_1 and λ_2 are the designed parameters for the controller. This parameter can be selected as procedure given in [17], [20]. After substituting the control input (8) into (7), we can get

$$\begin{aligned}\dot{x}_1 &= \hat{s} - c_1x_1 + e_2 \\ \dot{\hat{s}} &= c_1e_2 - \lambda_1|\hat{s}|^{\frac{1}{2}}\text{sign}(\hat{s}) - \int_0^t \lambda_2\text{sign}(\hat{s})d\tau + k_2\text{sign}(e_1).\end{aligned}\quad (9)$$

The overall closed loop system controller observer together can be represented as

$$\begin{aligned}\Pi : \begin{cases} \dot{x}_1 &= \hat{s} - c_1x_1 + e_2 \\ \dot{\hat{s}} &= c_1e_2 - \lambda_1|\hat{s}|^{\frac{1}{2}}\text{sign}(\hat{s}) - \int_0^t \lambda_2\text{sign}(\hat{s})d\tau + k_2\text{sign}(e_1) \end{cases} \\ \Xi : \begin{cases} \dot{e}_1 &= -k_1|e_1|^{\frac{1}{2}}\text{sign}(e_1) + e_2 \\ \dot{e}_2 &= -k_2\text{sign}(e_1) + \rho_1. \end{cases}\end{aligned}$$

It is already discussed earlier that estimation error of system Ξ converges to zero in finite time, i.e. there exists a $T_0 > 0$

such that for all $t > T_0$, it follows that $e_1 = e_2 = 0$. Note that the trajectories of system Π (above) cannot escape to infinity in finite time [25, Theorem 5.1]. Usually observer gains are chosen in such a way that observation error converges faster. After finite time $t > T_0$, the closed loop system further we can write as the following

$$\begin{aligned}\dot{x}_1 &= \hat{s} - c_1 x_1 \\ \dot{\hat{s}} &= -\lambda_1 |\hat{s}|^{\frac{1}{2}} \text{sign}(\hat{s}) - \int_0^t \lambda_2 \text{sign}(\hat{s}) d\tau + k_2 \text{sign}(e_1).\end{aligned}\quad (10)$$

In another way by adding some new fictitious state variable L we can represent dynamics as

$$\begin{aligned}\dot{x}_1 &= \hat{s} - c_1 x_1 \\ \dot{\hat{s}} &= -\lambda_1 |\hat{s}|^{\frac{1}{2}} \text{sign}(\hat{s}) + L + k_2 \text{sign}(e_1) \\ \dot{L} &= -\lambda_2 \text{sign}(\hat{s}).\end{aligned}\quad (11)$$

A. Discussion of the above Mathematical Transformation

Now, we can conclude from the above mathematical transformation, SOSM never achieved in (11), because $\dot{\hat{s}}$ contains the non-differentiable term $k_2 \text{sign}(e_1)$, which prevents the possibility of lower two equation of (11) to act as the STA. Thus second order sliding motion (so that $\hat{s} = \dot{\hat{s}} = 0$ in finite time) never begins. The block diagram of STC based on STO for system (1) is given in the Fig 1.

Next, we are going to propose the possible methodology of the control design such that non-differentiable term $k_2 \text{sign}(e_1)$ cancels out and then the lower two subsystems of (11) act as the STA and finally SOSM is established. For this purpose control is selected according to the following proposition,

Proposition 1. *The following control input leads to the establishment SOSM in finite time for (7), which further implies asymptotic stability of x_1 and x_2 ,*

$$u = -c_1 \hat{x}_2 - k_2 \text{sign}(e_1) - \lambda_1 |\hat{s}|^{\frac{1}{2}} \text{sign}(\hat{s}) - \int_0^t \lambda_2 \text{sign}(\hat{s}) d\tau,\quad (12)$$

where $\lambda_1 > 0$ and $\lambda_2 > 0$.

Proof. The system dynamics after substituting (12) into (7),

$$\begin{aligned}\dot{x}_1 &= \hat{s} - c_1 x_1 + e_2 \\ \dot{\hat{s}} &= c_1 e_2 - \lambda_1 |\hat{s}|^{\frac{1}{2}} \text{sign}(\hat{s}) - \int_0^t \lambda_2 \text{sign}(\hat{s}) d\tau.\end{aligned}\quad (13)$$

Now, the overall closed loop system can be represented as

$$\begin{aligned}\Pi_1 : \begin{cases} \dot{x}_1 &= \hat{s} - c_1 x_1 + e_2 \\ \dot{\hat{s}} &= c_1 e_2 - \lambda_1 |\hat{s}|^{\frac{1}{2}} \text{sign}(\hat{s}) - \int_0^t \lambda_2 \text{sign}(\hat{s}) d\tau \end{cases} \\ \Xi : \begin{cases} \dot{e}_1 &= -k_1 |e_1|^{\frac{1}{2}} \text{sign}(e_1) + e_2 \\ \dot{e}_2 &= -k_2 \text{sign}(e_1) + \rho_1. \end{cases}\end{aligned}\quad (14)$$

The observer error of system Ξ converges to zero in finite time which is discussed earlier. Note that the trajectories of system Π_1 (above) cannot escape to infinity in finite time [25,

Theorem 5.1]. So, we can substitute $e_2 = 0$, further we can write closed loop system as

$$\begin{aligned}\dot{x}_1 &= \hat{s} - c_1 x_1 \\ \dot{\hat{s}} &= -\lambda_1 |\hat{s}|^{\frac{1}{2}} \text{sign}(\hat{s}) + \nu \\ \dot{\nu} &= -\lambda_2 \text{sign}(\hat{s})\end{aligned}\quad (15)$$

where $\nu = -\int_0^t \lambda_2 \text{sign}(\hat{s}) d\tau$. The last two equations of (15) have the structure same as STA. Therefore, one can easily conclude that after finite time $t > T_1$, $\hat{s} = \dot{\hat{s}} = 0$. Later, the remaining system dynamics can be written as

$$\begin{aligned}\dot{x}_1 &= -c_1 x_1 \\ x_2 &= -c_1 x_1\end{aligned}\quad (16)$$

Therefore, both the states x_1 and x_2 are asymptotically stable by choosing $c_1 > 0$. The block diagram of the controller (12) based on STO is shown in the Fig 2. \square

It is clear from the mathematical derivation of the control (12) that, if one can uses STO to estimate the state of the second order uncertain system (1) and then design STC by selecting sliding manifold as (4), the control becomes discontinuous, because it contains the discontinuous term $k_2 \text{sign}(e_1)$. Therefore, continuous control design based on STO-STC is not possible. It is also to be noted that in this method only $|\rho_1| < \Delta_0$ is needed. Before, going to propose the solution of above mentioned problem, it is necessary to discuss the existing methodology of super-twisting output feedback (STOF) control.

III. SUPER-TWISTING OUTPUT FEEDBACK CONTROL

In the existing references it is reported that first consider the following sliding surface

$$s = c_1 x_1 + x_2\quad (17)$$

assuming that entire state vector is available. After that for realizing the control expression based on STA, take the first time derivative of sliding surface s (17),

$$\dot{s} = c_1 \dot{x}_1 + \dot{x}_2\quad (18)$$

Substituting \dot{x}_1 and \dot{x}_2 from (1) into (18), it follows that

$$\dot{s} = c_1 x_2 + u + \rho_1\quad (19)$$

Now, select control input u as

$$u = -c_1 x_2 - \lambda_1 |s|^{\frac{1}{2}} \text{sign}(s) - \int_0^t \lambda_2 \text{sign}(s) d\tau,\quad (20)$$

assuming both the states are available for measurement. After substituting the control (20) into (19), one can write

$$\dot{s} = -\lambda_1 |s|^{\frac{1}{2}} \text{sign}(s) - \int_0^t \lambda_2 \text{sign}(s) d\tau + \rho_1,\quad (21)$$

or

$$\begin{aligned}\dot{s} &= -\lambda_1 |s|^{\frac{1}{2}} \text{sign}(s) + z \\ \dot{z} &= -\lambda_2 \text{sign}(s) + \dot{\rho}_1.\end{aligned}\quad (22)$$

where $z = \nu_1 + \rho_1$ and $\nu_1 = -\int_0^t \lambda_2 \text{sign}(s) d\tau$. It is assumed that $|\dot{\rho}_1| < \Delta_1$. By selecting $\lambda_1 = 1.5\sqrt{\Delta_1}$ and $\lambda_2 = 1.1\Delta_1$

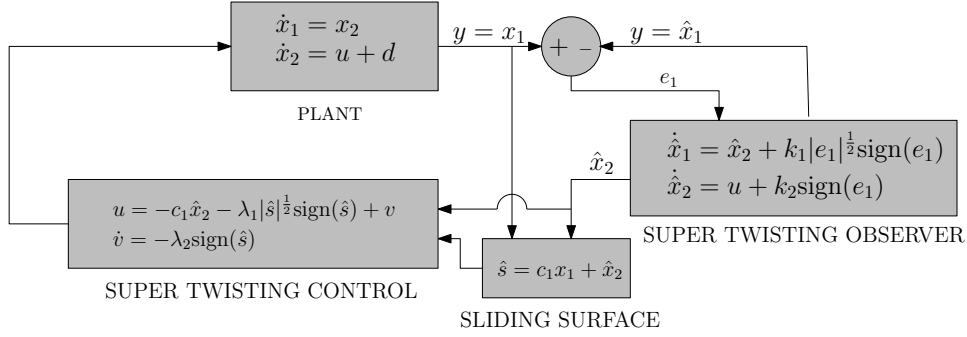


Fig. 1. Block diagram of the Super-twisting Control based on Super-twisting Observer

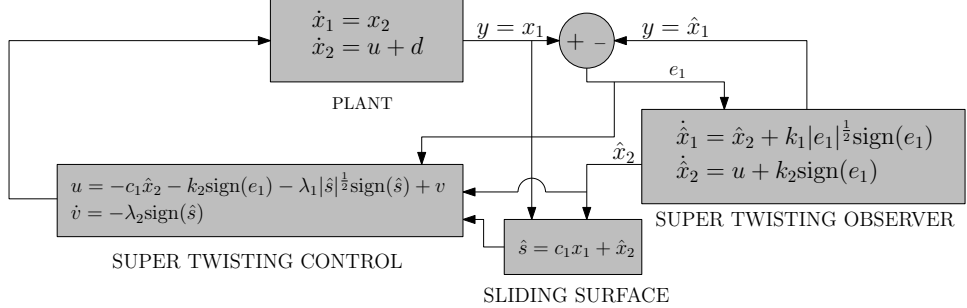


Fig. 2. Block diagram of the Proposition 1 control based on Super-twisting Observer

according to [17], [20], which leads to SOSM in finite time on s . Once $s = \dot{s} = 0$, then x_1 and x_2 both converge to zero asymptotically which is discussed in earlier section.

The control (20) is based on full state information, so we cannot implement it directly on system (1) because we do not have the information of x_2 . If we use STO to estimate the \hat{x}_2 and using it in control (20) by replacing x_2 with its estimated value \hat{x}_2 then control input (20) becomes,

$$u = -c_1\hat{x}_2 - \lambda_1|\hat{s}|^{\frac{1}{2}}\text{sign}(\hat{s}) - \int_0^t \lambda_2\text{sign}(\hat{s})d\tau, \quad (23)$$

where $\hat{s} = c_1x_1 + \hat{x}_2$. If the controller (23) is applied to (1) then it is not possible to get SOSM on the chosen surface. It is already shown in the section II that control input (8) which is same as (23) is not able to achieve SOSM on the sliding surface \hat{s} . If the control is applied to the system, then system becomes (11) where discontinuous term is presents in the first derivative of the sliding surface which prevents the SOSM on the chosen surface. So the method is not mathematically correct to get SOSM on chosen sliding surface.

Remark 1. *If we use this method for practical implementation it may work (which may not be true for all system), because most of the time controller implemented digitally through computer. It mean that controller is implemented at some fix sampling time, so the value of discontinuous term $k_2\text{sign}(e_1)$ will be constant during sampling interval.*

In STOF control approach one has to choose STO gains k_1 and k_2 based on the upper bound of the disturbance and STC gains λ_1 and λ_2 based on the upper bound of the derivative of the disturbance.

Now, in the next section we are going to proposed the new

strategy, which gives the correct way to implement STC, when only output information of the perturbed double integrator (1) is available.

IV. HOSMO BASED STC FOR PERTURBED DOUBLE INTEGRATOR SYSTEM

The dynamics of HOSMO to estimate the states of perturbed double integrator system (1) is given as

$$\begin{aligned} \dot{\hat{x}}_1 &= \hat{x}_2 + z_1 \\ \dot{\hat{x}}_2 &= \hat{x}_3 + u + z_2 \\ \dot{\hat{x}}_3 &= z_3, \end{aligned} \quad (24)$$

where z_1 , z_2 and z_3 are the correction terms. Let us define the error variable $e_1 = x_1 - \hat{x}_1$ and $e_2 = x_2 - \hat{x}_2$. The correction terms are defined as $z_1 = k_1|e_1|^{\frac{2}{3}}\text{sign}(e_1)$, $z_2 = k_2|e_1|^{\frac{1}{3}}\text{sign}(e_1)$ and $z_3 = k_3\text{sign}(e_1)$, where k_1 , k_2 and k_3 are the positive constant. Then, error dynamics can be written as

$$\begin{aligned} \dot{e}_1 &= -k_1|e_1|^{\frac{2}{3}}\text{sign}(e_1) + e_2 \\ \dot{e}_2 &= -k_2|e_1|^{\frac{1}{3}}\text{sign}(e_1) - \hat{x}_3 + \rho_1 \\ \dot{\hat{x}}_3 &= -k_3\text{sign}(e_1), \end{aligned} \quad (25)$$

Now, defining the new variable as $e_3 = -\hat{x}_3 + \rho_1$. We also assumed that disturbance ρ_1 is a Lipschitz and $|\dot{\rho}_1| < \Delta_1$. Then, further we can rewrite (25) as

$$\begin{aligned} \dot{e}_1 &= -k_1|e_1|^{\frac{2}{3}}\text{sign}(e_1) + e_2 \\ \dot{e}_2 &= -k_2|e_1|^{\frac{1}{3}}\text{sign}(e_1) + e_3 \\ \dot{e}_3 &= -k_3\text{sign}(e_1) + \dot{\rho}_1, \end{aligned} \quad (26)$$

The above equation is finite time stable which is already proved in literature [23], [24], so we can conclude that e_1 , e_2 and e_3 will converge to zero in finite time $t > T_2$, by selecting the appropriate gains k_1 , k_2 and k_3 [18]. After the convergence of error, one can find that $x_1 = \hat{x}_1$, $x_2 = \hat{x}_2$ and $\hat{x}_3 = \rho_1$ after finite time $t > T_2$.

Now, we will design a STC based on the estimated state information for a system (1). For that consider the same sliding surface (4) and taking its time derivative, it follows that,

$$\begin{aligned}\dot{\hat{s}} &= c_1 \dot{x}_1 + \dot{\hat{x}}_2 \\ \dot{\hat{s}} &= c_1 \hat{x}_2 + c_1 e_2 + u + k_2 |e_1|^{\frac{1}{3}} \text{sign}(e_1) + \int_0^t k_3 \text{sign}(e_1) d\tau\end{aligned}\quad (27)$$

Representing the system (1) in the co-ordinate of x_1 and \hat{s} by using (4) and (27), then we can write dynamics as

$$\begin{aligned}\dot{x}_1 &= \hat{s} - c_1 x_1 + e_2 \\ \dot{\hat{s}} &= c_1 \hat{x}_2 + c_1 e_2 + u + k_2 |e_1|^{\frac{1}{3}} \text{sign}(e_1) + \int_0^t k_3 \text{sign}(e_1) d\tau\end{aligned}\quad (28)$$

The main aim here, is to design a continuous control u , such that the SOSM occurs in finite time on the sliding surface. For this purpose control is selected according to the following proposition.

Proposition 2. *The following control input leads to the establishment of SOSM on \hat{s} in finite time, once $\hat{s} = 0$ it further implies asymptotic stability of x_1 and x_2 ,*

$$\begin{aligned}u &= -c_1 \hat{x}_2 - k_2 |e_1|^{\frac{1}{3}} \text{sign}(e_1) - \int_0^t k_3 \text{sign}(e_1) d\tau \\ &\quad - \lambda_1 |\hat{s}|^{\frac{1}{2}} \text{sign}(\hat{s}) - \int_0^t \lambda_2 \text{sign}(\hat{s}) d\tau\end{aligned}\quad (29)$$

or

$$\begin{aligned}u &= -c_1 \hat{x}_2 - \int_0^t k_3 \text{sign}(e_1) d\tau - \lambda_1 |\hat{s}|^{\frac{1}{2}} \text{sign}(\hat{s}) \\ &\quad - \int_0^t \lambda_2 \text{sign}(\hat{s}) d\tau\end{aligned}\quad (30)$$

where $\lambda_1 > 0$ and $\lambda_2 > 0$.

Proof. Substituting the control input (29) in the (28), we can get

$$\begin{aligned}\dot{x}_1 &= \hat{s} - c_1 x_1 + e_2 \\ \dot{\hat{s}} &= c_1 e_2 - \lambda_1 |\hat{s}|^{\frac{1}{2}} \text{sign}(\hat{s}) + v \\ \dot{v} &= -\lambda_2 \text{sign}(\hat{s}),\end{aligned}\quad (31)$$

Now, the overall closed loop system can be represented as

$$\begin{aligned}\Pi_2 : \begin{cases} \dot{\hat{x}}_1 &= \hat{s} - c_1 x_1 + e_2 \\ \dot{\hat{s}} &= c_1 e_2 - \lambda_1 |\hat{s}|^{\frac{1}{2}} \text{sign}(\hat{s}) + v \\ \dot{v} &= -\lambda_2 \text{sign}(\hat{s}), \end{cases} \\ \Xi_1 : \begin{cases} \dot{e}_1 &= -k_1 |e_1|^{\frac{2}{3}} \text{sign}(e_1) + e_2 \\ \dot{e}_2 &= -k_2 |e_1|^{\frac{1}{3}} \text{sign}(e_1) + e_3 \\ \dot{e}_3 &= -k_3 \text{sign}(e_1) + \dot{\rho}_1, \end{cases}\end{aligned}\quad (32)$$

It is already discussed earlier that estimation error of system Ξ_1 converges to zero in finite time. Note that the trajectories of system Π_2 (above) cannot escape to infinity in finite time [25, Theorem 5.1]. So, we can substitute $e_1 = e_2 = 0$. Once the error becomes zero, the closed loop system is given by the following expression

$$\begin{aligned}\dot{x}_1 &= \hat{s} - c_1 x_1 \\ \dot{\hat{s}} &= -\lambda_1 |\hat{s}|^{\frac{1}{2}} \text{sign}(\hat{s}) + v \\ \dot{v} &= -\lambda_2 \text{sign}(\hat{s})\end{aligned}\quad (33)$$

The lower two equation of (33) is a STA, by selecting appropriate gains $\lambda_1 > 0$ and $\lambda_2 > 0$, then $\hat{s} = \dot{\hat{s}} = 0$ in finite time, which further implies, that the closed loop system is given as

$$\begin{aligned}\dot{x}_1 &= -c_1 x_1 \\ \dot{x}_2 &= -c_1 x_1\end{aligned}\quad (34)$$

Therefore, both the states x_1 and x_2 are asymptotically stable by choosing $c_1 > 0$. The block diagram for super-twisting control based on HOSM observer is depicted in Fig 3. \square

A. Discussion of HOSMO based STC Design

It is clear from the STC control (29) and (30) expression based on HOSMO (24) is continuous. Also, when we design STC control based on HOSMO then one has to tune only the observer gains, according to the first derivative of disturbance, because it is necessary for the convergence of the error variables of the HOSMO. However, during controller design there is no explicit gain condition for the λ_2 with respect to the disturbances.

One can also observe that super-twisting output feedback controller (23) design based on super-twisting observer, requires two gains, one is STO gain means observer gain k_2 based on the explicit maximum bound of the direct disturbance and another is λ_2 , STC gain based on the maximum bound of the derivative of disturbance.

Therefore, one can conclude from the above observation that sound mathematical analysis reduces the two gains conditions with respect to disturbance by simply one gain condition. Also the precision of the sliding manifold is much improved by using the HOSMO based STC rather than STO based STC. Due to the increase of this precision of sliding variable precision of the states are also much affected. In other word if we talk about stabilization problem, then states are much closer to the origin in the case of HOSMO based STC rather than STO based STC. We only talk about the closeness of states variable with respect to an equilibrium point, because only asymptotic stability is possible in both the design methodology.

V. APPLICATION OF HOSMO BASED STC FOR THE POSITION CONTROL OF INDUSTRIAL EMULATOR

The industrial emulator system shown in Fig. 4 is an electromechanical system that represents the important classes of systems such as conveyors, machine tools, spindle drives, and automated assembly machines. The setup is provided by Educational Control Products (ECP) [31], California, USA.

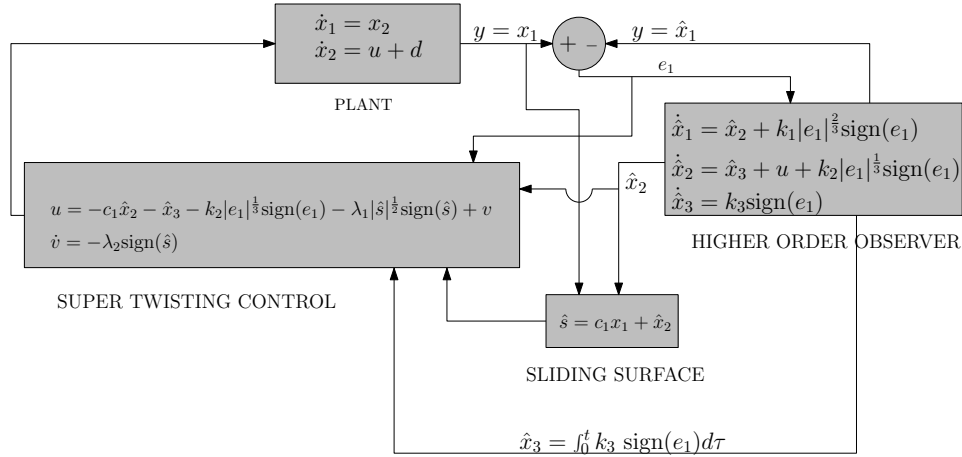


Fig. 3. Block diagram of the Super-twisting Control based on HOSM Observer

The system consists of a drive disk which is driven through a drive motor (servo actuator). The drive disk is coupled to the drive motor through a timing belt. The motion of the drive disk is transferred to another disk called load disk which is used to load the system. The motion from drive disk to load disk is transferred through a speed reduction assembly (idler pulleys) and a timing belt. The load and the drive disk inertias are adjustable. High resolution encoder is used to measure the position of the drive disk and load disk. The drive motor is driven by a servo amplifier. The system equation in state space

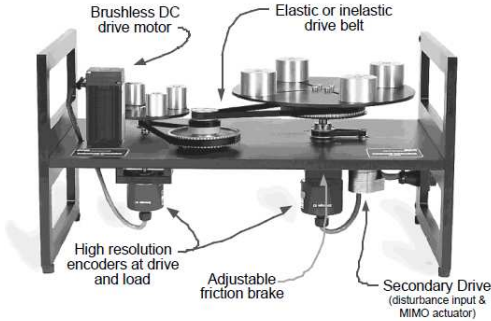


Fig. 4. Industrial Emulator Setup [31]

form is given by

$$\begin{bmatrix} \dot{x}_1 \\ \dot{x}_2 \end{bmatrix} = \begin{bmatrix} 0 & 1 \\ 0 & -8.4344 \end{bmatrix} \begin{bmatrix} x_1 \\ x_2 \end{bmatrix} + \begin{bmatrix} 0 \\ 458.46 \end{bmatrix} (u + d)$$

$$y = \begin{bmatrix} 1 & 0 \end{bmatrix} \begin{bmatrix} x_1 \\ x_2 \end{bmatrix} \quad (35)$$

where x_1, x_2 are the angular position and the angular velocity of the load disk, u is the input voltage to the drive motor and d is the disturbance voltage signal injected externally to perturb the plant.

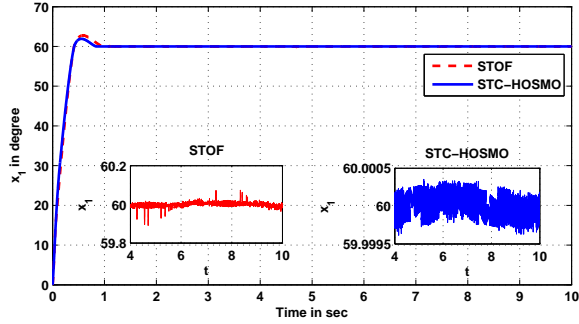
For the simulation and experimental result $d = 0.2 \sin(t)$ is chosen. The control input in proposition 1 is discontinuous which is not good for practical setup, So we have compared the two control techniques STOF and STC based on HOSMO

for the implementation. The controller and observer gains are selected as follows

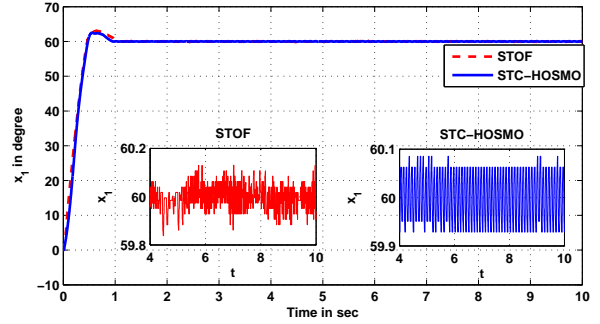
- STOF
 - STC gains $\lambda_1 = 2$ and $\lambda_2 = 2$
 - STO gains $k_1 = 1.5\sqrt{m}$ and $k_2 = 1.1m$, where $m = 100$.
- STC-HOSMO
 - STC gains $\lambda_1 = 2$ and $\lambda_2 = 2$
 - HOSMO gains $k_1 = 6n^{1/3}$, $k_2 = 11n^{1/2}$ and $k_3 = 6n$, where $n = 50$.

The sliding surface is chosen as $\hat{s} = x_1 + \frac{1}{458.46} \hat{x}_2$. The controller and observer is implemented in MATLAB with sampling time 1ms. Control objective is to bring the load disk from zero position to the desired position, we have selected 60 degree as the desired position. The simulation and experimental results comparison of STOF and STC-HOSMO methods are illustrated in the Fig.5 and Fig.6. One can see the both method achieves desired load disk position, but from zoom version we can say that precision of position in STC-HOSMO is more compare to STOF. The experimental results for the same is shown in Fig.5(b). Fig.5(c) and (d) shows the simulation and experimental results of estimated states using STO and HOSMO. One can see the estimated state using HOSMO is more correct than the STO. The control input plot in simulation and experimental is depicted in Fig.5(e) and (f) respectively.

From the observation one can say that control input is more smoother in the case of STC-HOSMO compare to STOF. The sliding surface simulation plot is shown in the Fig.6(a), one can see that precision of the sliding variable (in zoom plot) is more (up to the order of τ^2) in the case of STC-HOSMO, while in the case of STOF precision is only the order of τ . So, we can say that in STOF method we are not able to get exact second order sliding mode, but in STC-HOSMO we are getting the exact second order sliding mode on the sliding surface. The plot of sliding surface in experiment is depicted in Fig.6(b). The evolution of observer error in simulation and experiment are shown in the Fig.6(c) and (d). The precision of error in HOSMO is more compared to STO that we can



(a) Evolution of position (simulation)



(b) Evolution of position (experimental)

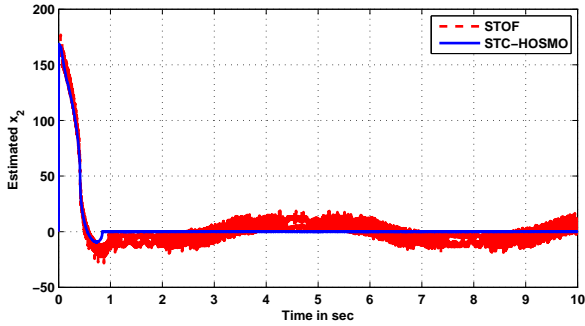
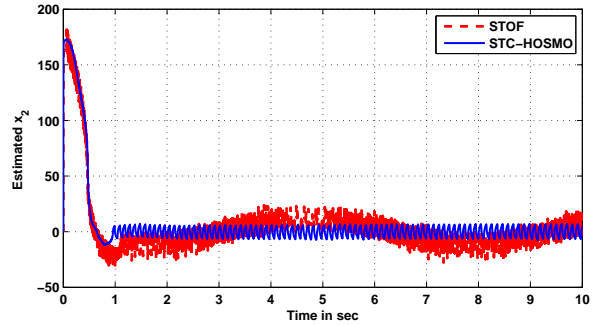
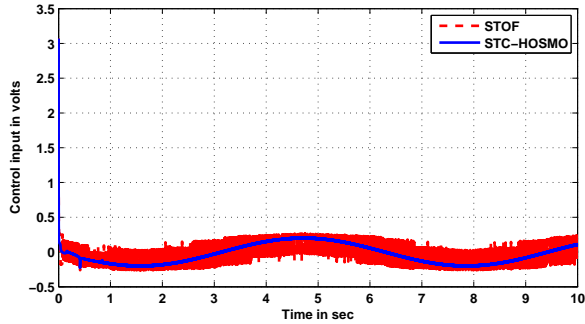
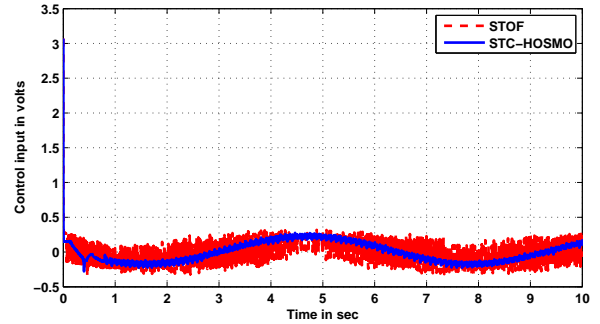
(c) Evolution of estimated state x_2 (simulation)(d) Evolution of estimated state x_2 (experimental)(e) Evolution of control input u (simulation)(f) Evolution of control input u (experimental)

Fig. 5. Simulation and Experimental Results: Industrial Plant Emulator

see from the zoom version.

VI. CONCLUSION

It is shown in the paper that when STC is implemented based on super-twisting observer (STO) then it is not possible to achieve second order sliding mode (SOSM) using continuous control on the chosen sliding surface. Two methodologies are proposed to circumvent the above mentioned problem. For simplicity, here only the perturbed double integrator is considered, which can be generalized for an arbitrary order. Numerical simulations and experimental validation are also presented to show the effectiveness of the proposed method.

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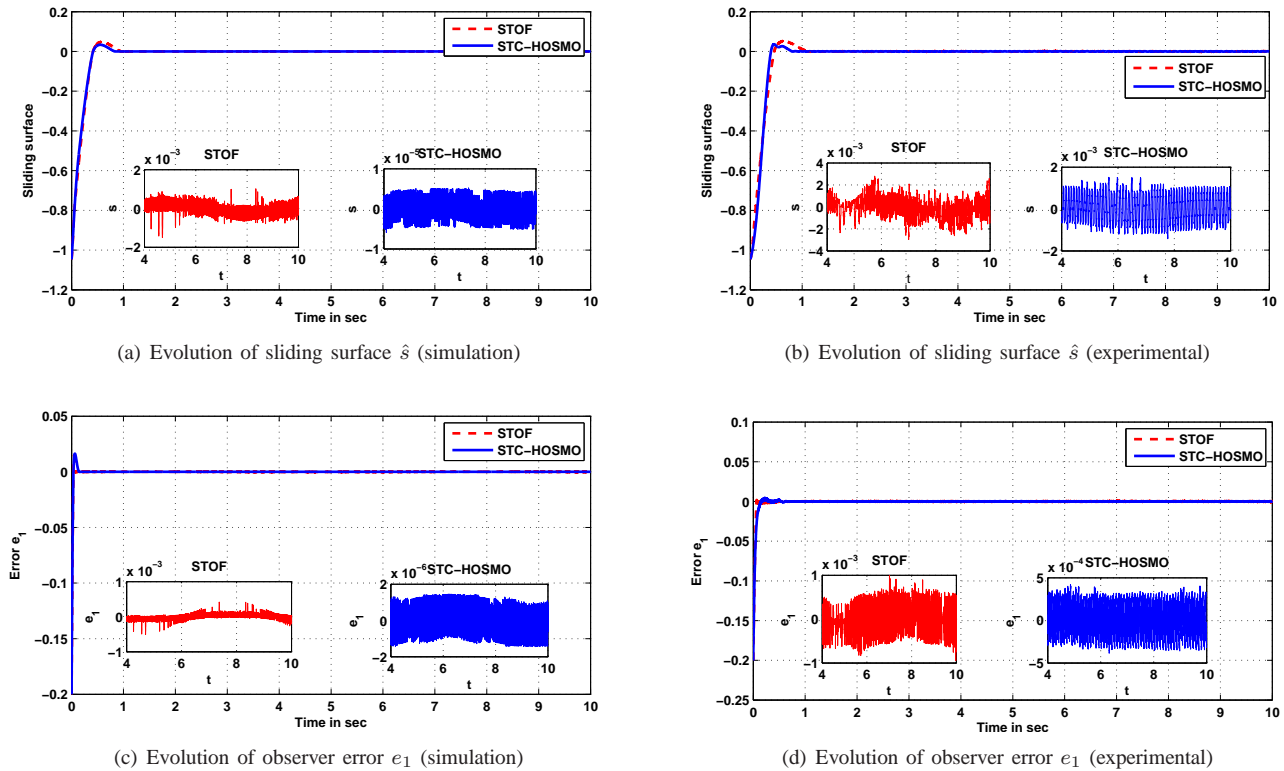


Fig. 6. Simulation and Experimental Results: Industrial Plant Emulator

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Asif Chalanga (M'16) received his Bachelors degree in Electrical Engineering from the University of Bhavnagar, India in 2007, M.Tech in Control Systems from College of Engineering Pune, India in 2010 and Ph.D. in Systems and Control Engineering at Indian Institute of Technology Bombay, India in 2015. His research interests include the areas of discrete and continuous higher order sliding mode control and application aspects of the sliding mode to real time systems.



Shyam Kamal (M'15) received his Bachelors degree in Electronics and Communication Engineering from the Gurukula Kangri Vishwavidyalaya Haridwar, Utrakhand, India in 2009, and Ph.D. in Systems and Control Engineering from the Indian Institute of Technology Bombay, India in 2014. Currently he is a project assistant professor at Department of Systems Design and Informatics, Kyushu Institute of Technology. He has published one monograph and 30 journal articles and conference papers. His research interests include the areas of fractional

order systems, contraction analysis, discrete and continuous higher order sliding mode control.



Leonid M. Fridman (M'98) received an M.S. degree in mathematics from Kuibyshev (Samara) State University, Samara, Russia, in 1976, a Ph.D. degree in applied mathematics from the Institute of Control Science, Moscow, Russia, in 1988, and a Dr. Sc. degree in control science from Moscow State University of Mathematics and Electronics, Moscow, Russia, in 1998. From 1976 to 1999, he was with the Department of Mathematics, Samara State Architecture and Civil Engineering University. From 2000 to 2002, he was with the Department

of Postgraduate Study and Investigations at the Chihuahua Institute of Technology, Chihuahua, Mexico. In 2002, he joined the Department of Control Engineering and Robotics, Division of Electrical Engineering of Engineering Faculty at National Autonomous University of Mexico (UNAM), Mexico. His research interests are Variable Structure Systems. He is currently a Chair of TC on Variable Structure Systems and Sliding mode control of IEEE Control Systems Society, Associated Editor of the Journal of Franklin Institute, and Nonlinear Analysis: Hybrid Systems. He is an author and editor of eight books and fifteen special issues devoted to the sliding mode control. He is a winner of Scopus prize for the best cited Mexican Scientists in Mathematics and Engineering 2010. He was working as an invited professor in 20 universities and research laboratories of Argentina, Australia, Austria, China, France, Germany, Italy, Israel, and Spain.



Bijnan Bandyopadhyay (SM'06) received his B.E. degree in Electronics and Telecommunication Engineering from the University of Calcutta, Calcutta, India in 1978, and Ph.D. in Electrical Engineering from the Indian Institute of Technology Delhi, India in 1986. In 1987, he joined the Interdisciplinary Programme in Systems and Control Engineering, Indian Institute of Technology Bombay, India, as a faculty member, where he is currently a Professor. In 1996, he was with the Lehrstuhl für Elektrische Steuerung und Regelung, Ruhr Universität Bochum,

Bochum, Germany, as an Alexander von Humboldt Fellow. He has been a visiting Professor at Okayama University, Japan, Korea Advance Institute Science and Technology (KAIST) S.Korea and Chiba National University in 2007. He visited University of Western Australia, Australia as a Gladden Visiting Senior Fellow in 2007. Professor Bandyopadhyay is recipient of UKIERI(UK India Education and Research Initiative) Major Award in 2007, 'Distinguished Visiting Fellowship' award in 2009 and 2012 from "The Royal Academy of Engineering", London. Professor Bandyopadhyay is a Fellow of Indian National Academy of Engineering (INAE), Senior member of IEEE and a Fellow of IETE (India). He has published ten books and monographs, ten book chapters and more than 340 journal articles and conference papers. He has guided 30 Ph.d. thesis at IIT Bombay. His research interests include the areas of higher order sliding mode control, multirate output feedback control, discrete-time sliding mode control, large-scale systems, model order reduction, nuclear reactor control and smart structure control. Prof. Bandyopadhyay served as Co-Chairman of the International Organization Committee and as Chairman of the Local Arrangements Committee for the IEEE International Conference in Industrial Technology, held in Goa, India, in Jan. 2000. He also served as one of the General Chairs of IEEE ICIT conference held in Mumbai, India in December 2006. Prof. Bandyopadhyay has served as General Chair for IEEE International Workshop on Variable Structure Systems held in Mumbai in January 2012.



Jaime Moreno (M'97) was born in Colombia and he received his PhD degree (Summa cum Laude) in Electrical Engineering (Automatic Control) from the Helmut-Schmidt University in Hamburg, Germany in 1995. The Diplom-Degree in Electrical Engineering (Automatic Control) from the Universität zu Karlsruhe, Karlsruhe, Germany in 1990, and the Licentiate-Degree (with honors) in Electronic Engineering from the Universidad Pontificia Bolivariana, Medellín, Colombia in 1987. He is full Professor of Automatic Control and the Head of

the Electrical and Computing Department at the Institute of Engineering from the National University of Mexico (UNAM), in Mexico City. He is member of the Technical Board of IFAC. He is the author and editor of 8 books, 4 book chapters, 1 patent, and author and co-author of more than 300 papers in refereed journals and conference proceedings. His current research interests include robust and non-linear control with application to biochemical processes (wastewater treatment processes), the design of nonlinear observers and higher order sliding mode control.